

DEVELOPMENT OF CIRCUITS AND SYSTEM MODELS FOR THE SYNCHRONIZATION OF THE ILC CRAB CAVITIES

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Abstract

The ILC reference design report (RDR) recommends a 14 mrad crossing angle for the positron and electron beams at the IP. A matched pair of crab cavity systems are required in the beam delivery system to align both bunches at the IP. The use of a multi-cell, 3.9 GHz dipole mode superconducting cavity is proposed, derived from the Fermilab CKM cavity being developed as a beam slice diagnostic [1]. Dipole-mode cavities phased for crab rotation are shifted by 90° with respect to similar cavities phased for deflection. Uncorrelated phase errors of 0.086° (equivalent to 61 fs) for the two cavity systems, gives an average of 180 nm for the relative deflection of the bunch centers. For a horizontal bunch size $\sigma_x = 655$ nm, a deflection of 180 nm reduces the ILC luminosity by 2%. The crab cavity systems are to be placed ~ 30 m apart and synchronization to within 61 fs is required; this is on the limit of what is presently achievable. This paper describes LLRF circuits under development at the Cockcroft Institute for proof of principle experiments planned on the ERLP at Daresbury and on the ILCTA test beamline at FNAL. Simulation results for stabilisation performance are also given.

PRELIMINARY LLRF LAYOUT

There are a wide range of possible technologies and configurations that might be used for the crab cavity LLRF system. The circuits being developed are for proof of principle. Important criteria for the current system are flexibility and accurate synchronisation in the absence of beam based calibration. For superconducting cavities, the microphonics which act to spoil phase synchronism are independent for each cavity. Accordingly we chose separate amplifiers and controllers for each cavity. In order to synchronize the crab cavities we must therefore provide accurately synchronized timing signals very close to the output couplers of each cavity. The cavities then need to be stabilized with respect to the local timing signal. The timing error between cavity phases has three components, one from the synchronization of the timing signals and two from the cavity to timing signal synchronization. Our initial target is a cavity to a timing signal synchronization of 20 fs and a timing signal to timing signal synchronization also of 20 fs. Timing synchronization of 10 fs has recently been claimed at LBLN using mode locked lasers [2]. Our current system uses an RF interferometer which is not expected to achieve this performance but which could be easily replaced with such a system. The development system sketched in figure 1 employs digital phase detection permitting absolute measurement with minimal

calibration issues, 16 bit A to D conversion at 100 MSPS, DSP control algorithm implementation giving maximum flexibility and IQ modulation of the RF drive.

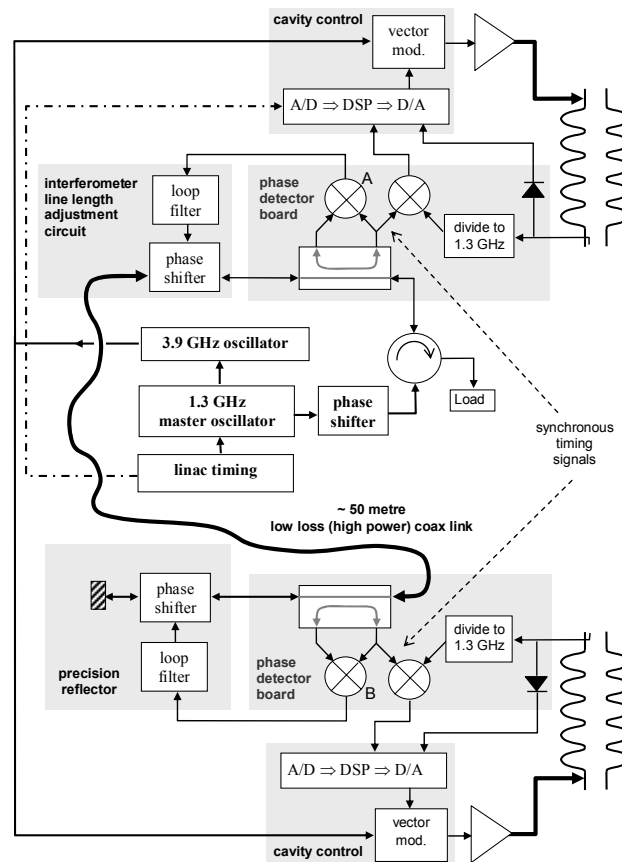


Figure 1: Synchronization layout.

CAVITY MODEL

The accuracy to which the phase of each cavity can be stabilized against unpredictable components of the disturbing influences of microphonics and beam-loading, will depend on how accurately the phase can be measured and the maximum control system gain consistent with stability. High gain RF control stability of the TESLA cavities has recently been discussed by Vogel [3]. The gain stability limit for the control system will depend on loop delay. For an analogue control loop, delay will arise from input filtering and amplifier bandwidth. For the digital control system being proposed here, control loop delay depends additionally on ADC, DAC and DSP processing time. Compensation for the additional loop delay of a digital controller is made by opportunities for sophisticated input filtering, real time variation of control parameters and anticipation of repetitive disturbances.

Calculation indicates that to get the required performance, digital processing delay needs to be less than about 1 μ s.

The anticipated performance of the control system can be modelled numerically. We apply the standard equations for cavity filling and numerically integrate the envelope equations [4] for anticipated microphonics and worst case beam-loading. Figure 2 shows the effective (diagonalized) equivalent circuit for a multi-cell cavity driven via a coupler. Values L_i , R_i , C_i are chosen so that each parallel resonator represents a cavity mode and are determined from modal frequencies, Q and R/Q values.

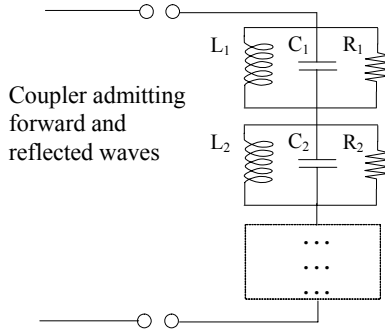


Figure 2: Cavity model.

One therefore solves

$$\frac{d^2 V_m}{dt^2} + \frac{\omega_m}{Q_{om}} \frac{dV_m}{dt} + \frac{1}{Q_{em}} \omega_m \sum_{j=1}^N \frac{dV_j}{dt} + \omega_m^2 V_m = \frac{2\omega_m}{Q_{em}} \frac{d}{dt} \{ \mathcal{F} \exp(-j\omega t) \}$$

where V_m , ω_m , Q_{om} and Q_{em} are the voltage, frequency, unloaded Q and Q external for the m^{th} mode respectively and \mathcal{F} is the amplitude of the forward wave in the coupler, ω is the drive frequency. This set of equations must be solved numerically as the modal frequencies are functions of time as determined by microphonics and the modal voltages take a step change each time a bunch passes through the cavity. These equations cannot be accurately integrated over the fill time and bunch train time which amounts to at least 10^7 RF cycles. Instead one solves for the real and imaginary parts of an amplitude function [4] determined by the equation

$$V_m(t) = \{ A_{mr}(t) + jA_{mi}(t) \} \exp\{-j\omega t\}$$

After neglecting second time derivatives of the slowly varying amplitude functions A_{mr} and A_{ri} and also terms of order $(1/Q_e)^2$ one obtains the envelope equations

$$\begin{aligned} \frac{\dot{A}_{mr}}{\omega_m} + \frac{1}{4Q_{om}} \left(\frac{\omega_m^2}{\omega^2} + 1 \right) A_{mr} + \frac{1}{4Q_{em}} \sum_{j=1}^N \left(\frac{\omega_j^2}{\omega^2} + 1 \right) A_{jr} \\ - \left(\frac{\omega_m}{\omega} - \frac{\omega}{\omega_m} \right) \frac{A_{mi}}{2} = -\frac{1}{Q_{em}} \left(\frac{\dot{\mathcal{F}}_i}{\omega} - \mathcal{F}_r \right) \\ \frac{\dot{A}_{mi}}{\omega_m} + \frac{1}{4Q_{om}} \left(\frac{\omega_m^2}{\omega^2} + 1 \right) A_{mi} + \frac{1}{4Q_{em}} \sum_{j=1}^N \left(\frac{\omega_j^2}{\omega^2} + 1 \right) A_{ji} \\ + \left(\frac{\omega_m}{\omega} - \frac{\omega}{\omega_m} \right) \frac{A_{mr}}{2} = \frac{1}{Q_{em}} \left(\frac{\dot{\mathcal{F}}_r}{\omega} + \mathcal{F}_i \right) \end{aligned}$$

For the planned 9 cell cavity, modes will be designated as mode = $\pi(1 - m/9)$ so that $m = 0$ gives the π mode.

The real and imaginary parts of the forward wave are determined by the controller which must reduce A_{0i} to zero and hold A_{0r} at a steady level V_{sp} as appropriate for required kick. At this stage we have no detailed knowledge of system disturbances hence use of a proportional integral controller is appropriate for the model. Explicitly we take

$$\mathcal{F}_r(t + t_{\text{delay}}) = c_{pr} \left(V_{sp} - \sum_m A_{mr} \right) + c_{ir} \int_{-\infty}^t dt \left(V_{sp} - \sum_m A_{mr} \right)$$

$$\mathcal{F}_i(t + t_{\text{delay}}) = -c_{pi} \sum_m A_{mi} - c_{ii} \int_{-\infty}^t dt \sum_m A_{mi}$$

where c_{pr} , c_{pi} , c_{ir} and c_{ii} are the controller coefficients and t_{delay} represents time delays in the digital processor. One wishes to control the π mode, however the measured cavity voltage will be some weighted time average of the summed excitation of the modes. As the weightings for this average have yet to be determined, the modes are sampled with equal weight through a low pass filter having a time constant equal to the sampling rate. The amplifier is modelled as a second order filter with a time constant determined from its bandwidth. Beamloading of the π mode with the ILC time structure is included. Wakefield calculations have shown that excitation of other modes by the beam is small. Monochromatic cavity vibration appropriate to the most prominent frequency measure on prototype CKM cavities is included.

RESULTS

Figures 3-7 show cavity voltage, drive amplitude and cavity phase during cavity filling and the passage of an ILC bunch train with an offset of 0.6 mm after 4.5 million 3.9 GHz, RF cycles. In this calculation only the cavity π mode is modelled. Phase measurement errors are not included. The cavity has a microphonic frequency of 230 Hz which shifts the RF frequency by 600 Hz. The ‘‘in phase’’ drive amplitude follows the beam loading whilst the ‘‘phase quadrature’’ drive amplitude compensates for microphonics as expected. If the beam offset is permitted to oscillate, then for perfect bunch timing the phase response remains as in figure 7. Figure 8 shows the influence of bunch timing errors when the bunch offset oscillates at 2 kHz. Figures 9 and 10 show the effect of including the $8\pi/9$ mode at +2.2 MHz and the $7\pi/9$ mode at +8.9 MHz in addition to the π mode at 3.9 GHz. Interestingly, beam-loading is seen to couple to the phase error when additional modes are included in the model. Note that the amplifier bandwidth was taken as 10 MHz. The gain was 36% below the point of instability [5]. Figure 10 represents a worst case control scenario in the absence of phase measurement errors. Using digital phase detectors and a loop bandwidth appropriate to the model, the measurement jitter after division to 1.3 GHz will be of the order of 10 milli-degrees.

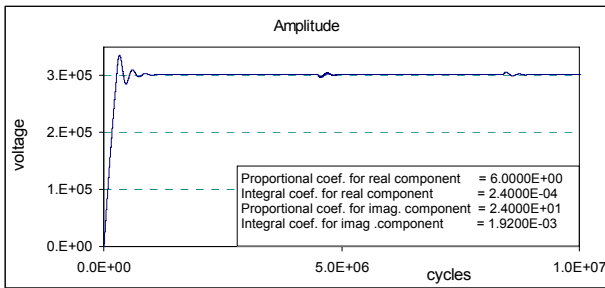


Figure 3 One mode and steady 0.6 mm beam offset

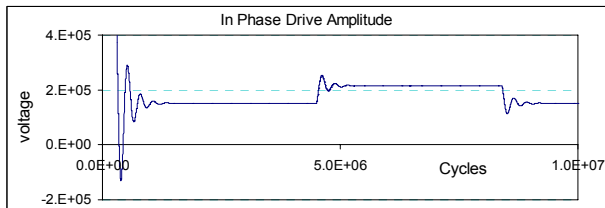


Figure 4 One mode and steady 0.6 mm beam offset

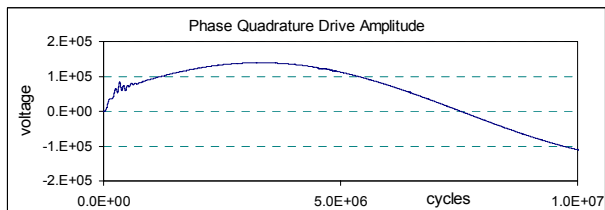


Figure 5 One mode and steady 0.6 mm beam offset

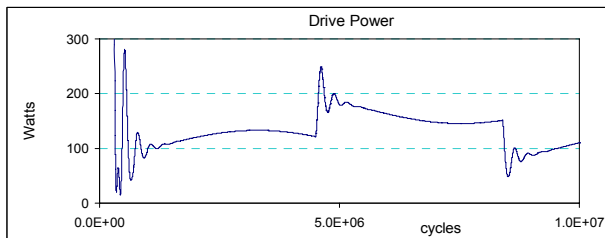


Figure 6 One mode and steady 0.6 mm beam offset

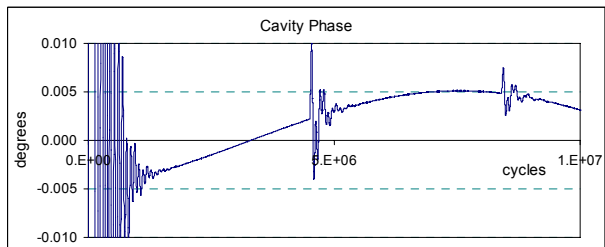


Figure 7 One mode and steady 0.6 mm beam offset

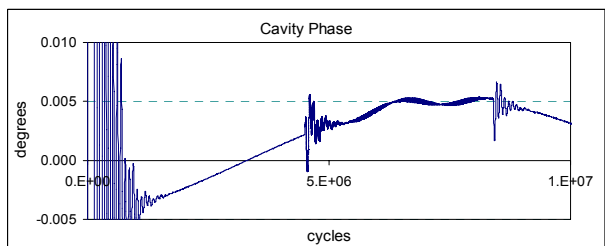


Figure 8 One mode and 0.6 mm oscillating beam offset and with 712 fs random, bunch timing errors

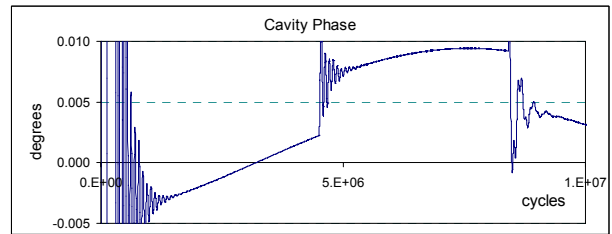


Figure 9 Three modes and 0.6mm beam offset

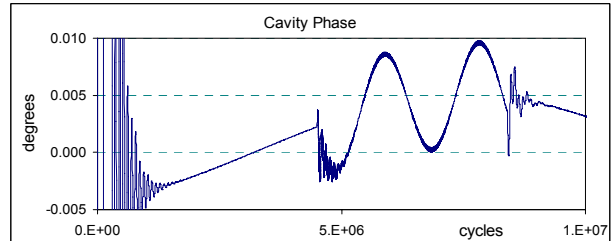


Figure 10 Three modes and 0.6mm oscillating beam offset with 712 fs random, bunch timing errors

Modelling has also been undertaken with measurements errors included and to a rough approximation they can be simply added to the results displayed. Taking contributions together, stabilization to 20 fs ~ 30 milli-degrees looks feasible.

FUTURE WORK

The LLRF circuits are soon to be tested by driving two adjacent cavities, independently in a vertical cryostat. As the cavities are adjacent it will be possible to make an independent measurement of relative cavity phase jitter.

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